



**THE DATASHEET OF  
MC34067DWG**



# MC34067, MC33067, NCV33067

## High Performance Resonant Mode Controllers

The MC34067/MC33067 are high performance zero voltage switch resonant mode controllers designed for off-line and dc-to-dc converter applications that utilize frequency modulated constant off-time or constant deadtime control. These integrated circuits feature a variable frequency oscillator, a precise retriggerable one-shot timer, temperature compensated reference, high gain wide bandwidth error amplifier, steering flip-flop, and dual high current totem pole outputs ideally suited for driving power MOSFETs.

Also included are protective features consisting of a high speed fault comparator and latch, programmable soft-start circuitry, input undervoltage lockout with selectable thresholds, and reference undervoltage lockout. These devices are available in dual-in-line and surface mount packages.

### Features

- Zero Voltage Switch Resonant Mode Operation
- Variable Frequency Oscillator with a Control Range Exceeding 1000:1
- Precision One-Shot Timer for Controlled Off-Time
- Internally Trimmed Bandgap Reference
- 4.0 MHz Error Amplifier
- Dual High Current Totem Pole Outputs
- Selectable Undervoltage Lockout Thresholds with Hysteresis
- Enable Input
- Programmable Soft-Start Circuitry
- Low Startup Current for Off-Line Operation
- NCV Prefix for Automotive and Other Applications Requiring Unique Site and Control Change Requirements; AEC-Q100 Qualified and PPAP Capable
- These Devices are Pb-Free, Halogen Free/BFR Free and are RoHS Compliant

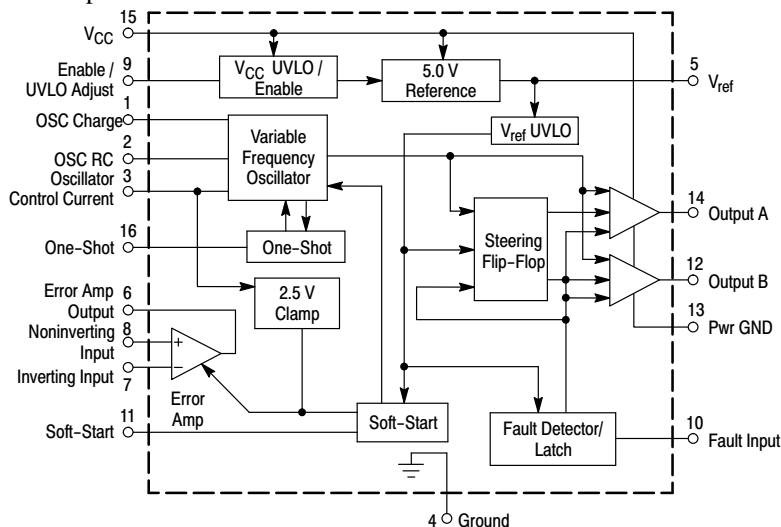


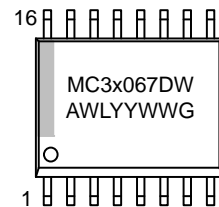
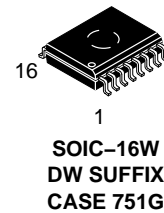
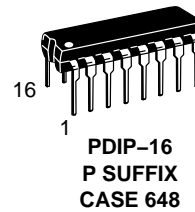
Figure 1. Simplified Block Diagram



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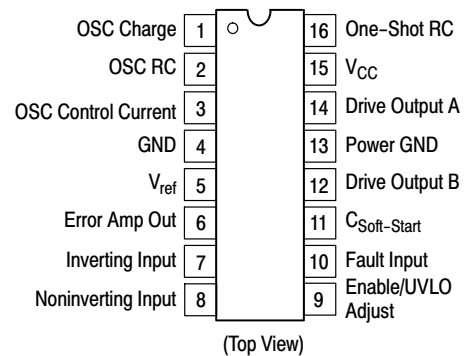
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### MARKING DIAGRAMS



x = 3 or 4  
A = Assembly Location  
WL = Wafer Lot  
YY = Year  
WW = Work Week  
G = Pb-Free Package

### PIN CONNECTIONS



### ORDERING INFORMATION

See detailed ordering and shipping information in the package dimensions section on page 2 of this data sheet.

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## MAXIMUM RATINGS

Rating	Symbol	Value	Unit
Power Supply Voltage	$V_{CC}$	20	V
Drive Output Current, Source or Sink (Note 1) – Continuous – Pulsed (0.5 $\mu$ s), 25% Duty Cycle	$I_O$	0.3 1.5	A
Error Amplifier, Fault, One-Shot, Oscillator and Soft-Start Inputs	$V_{in}$	– 1.0 to + 6.0	V
UVLO Adjust Input	$V_{in(UVLO)}$	– 1.0 to $V_{CC}$	V
Power Dissipation and Thermal Characteristics DW Suffix, Plastic Package, Case 751G $T_A = 25^\circ\text{C}$ Thermal Resistance, Junction-to-Air P Suffix, Plastic Package, Case 648 $T_A = 25^\circ\text{C}$ Thermal Resistance, Junction-to-Air	$P_D$ $R_{\theta JA}$ $P_D$ $R_{\theta JA}$	862 145 1.25 100	mW $^\circ\text{C/W}$ W $^\circ\text{C/W}$
Operating Junction Temperature	$T_J$	+ 150	$^\circ\text{C}$
Operating Ambient Temperature MC34067 MC33067, NCV33067	$T_A$	0 to + 70 – 40 to + 85	$^\circ\text{C}$
Storage Temperature	$T_{stg}$	– 55 to + 150	$^\circ\text{C}$
ESD Capability, HBM Model per JEDEC JESD22–A114F	–	2.0	kV
ESD Capability, CDM Model per JEDEC JESD22–C101E	–	1.0	kV

Stresses exceeding those listed in the Maximum Ratings table may damage the device. If any of these limits are exceeded, device functionality should not be assumed, damage may occur and reliability may be affected.

NOTE: This device contains latch-up protection and exceeds 100 mA per JEDEC Standard JESD78.

## ORDERING INFORMATION

Device	Package	Shipping <sup>†</sup>
MC33067DWG	SOIC–16W (Pb–Free)	47 Units / Rail
MC33067DWR2G	SOIC–16W (Pb–Free)	1000 / Tape & Reel
NCV33067DWR2G*	SOIC–16W (Pb–Free)	1000 / Tape & Reel
MC33067PG	PDIP–16 (Pb–Free)	25 Units / Rail
MC34067DWG	SOIC–16W (Pb–Free)	47 Units / Rail
MC34067DWR2G	SOIC–16W (Pb–Free)	1000 / Tape & Reel
MC34067PG	PDIP–16 (Pb–Free)	25 Units / Rail

<sup>†</sup>For information on tape and reel specifications, including part orientation and tape sizes, please refer to our Tape and Reel Packaging Specifications Brochure, BRD8011/D.

\*NCV Prefix for Automotive and Other Applications Requiring Unique Site and Control Change Requirements; AEC–Q100 Qualified and PPAP Capable.

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## ELECTRICAL CHARACTERISTICS

( $V_{CC} = 12\text{ V}$  [Note 2],  $R_{OSC} = 18.2\text{ k}$ ,  $R_{VFO} = 2940\ \Omega$ ,  $C_{OSC} = 300\text{ pF}$ ,  $R_T = 2370\ \Omega$ ,  $C_T = 300\text{ pF}$ ,  $C_L = 1.0\text{ nF}$ . For typical values  $T_A = 25^\circ\text{C}$ , for min/max values  $T_A$  is the operating ambient temperature range that applies (Note 3), unless otherwise noted.)

Characteristic	Symbol	Min	Typ	Max	Unit
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### REFERENCE SECTION

Reference Output Voltage ( $I_O = 0\text{ mA}$ , $T_J = 25^\circ\text{C}$ )	$V_{ref}$	5.0	5.1	5.2	V
Line Regulation ( $V_{CC} = 10\text{ V to } 18\text{ V}$ )	$Reg_{line}$	–	1.0	20	mV
Load Regulation ( $I_O = 0\text{ mA to } 10\text{ mA}$ )	$Reg_{load}$	–	1.0	20	mV
Total Output Variation Over Line, Load, and Temperature	$V_{ref}$	4.9	–	5.3	V
Output Short Circuit Current ( $0^\circ\text{C to } 70^\circ\text{C}$ ) ( $-40^\circ\text{C to } 85^\circ\text{C}$ )	$I_O$	30 25	100 100	190 225	mA
Reference Undervoltage Lockout Threshold	$V_{th}$	3.8	4.3	4.8	V

### ERROR AMPLIFIER

Input Offset Voltage ( $V_{CM} = 1.5\text{ V}$ )	$V_{IO}$	–	1.0	10	mV
Input Bias Current ( $V_{CM} = 1.5\text{ V}$ )	$I_{IB}$	–	0.2	1.0	$\mu\text{A}$
Input Offset Current ( $V_{CM} = 1.5\text{ V}$ )	$I_{IO}$	–	0	0.5	$\mu\text{A}$
Open Loop Voltage Gain ( $V_{CM} = 1.5\text{ V}$ , $V_O = 2.0\text{ V}$ )	$A_{VOL}$	70	100	–	dB
Gain Bandwidth Product ( $f = 100\text{ kHz}$ ) $T_A = 25^\circ\text{C}$ $T_A = T_{low}\text{ to } T_{high}$	GBW	3.0 2.7	5.0 –	– –	MHz
Input Common Mode Rejection Ratio ( $V_{CM} = 1.5\text{ V to } 5.0\text{ V}$ )	CMR	70	95	–	dB
Power Supply Rejection Ratio ( $V_{CC} = 10\text{ V to } 18\text{ V}$ , $f = 120\text{ Hz}$ )	PSR	80	100	–	dB
Output Voltage Swing High State ( $I_{source} = 2.0\text{ mA}$ ) Low State ( $I_{sink} = 4.0\text{ mA}$ )	$V_{OH}$ $V_{OL}$	2.8 –	3.2 0.6	– 0.8	V

Product parametric performance is indicated in the Electrical Characteristics for the listed test conditions, unless otherwise noted. Product performance may not be indicated by the Electrical Characteristics if operated under different conditions.

1. Maximum package power dissipation limits must be observed.
2. Adjust  $V_{CC}$  above the Startup Threshold voltage before setting to 12 V.
3. Low duty cycle pulse techniques are used during test to maintain junction temperature as close to ambient as possible.
4.  $T_{low} = 0^\circ\text{C}$  for MC34067  
 $= -40^\circ\text{C}$  for MC33067, NCV33067  
 $T_{high} = +70^\circ\text{C}$  for MC34067  
 $= +85^\circ\text{C}$  for MC33067, NCV33067

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**ELECTRICAL CHARACTERISTICS (continued)** ( $V_{CC} = 12\text{ V}$  [Note 6],  $R_{OSC} = 18.2\text{ k}$ ,  $R_{VFO} = 2940\ \Omega$ ,  $C_{OSC} = 300\text{ pF}$ ,  $R_T = 2370\ \Omega$ ,  $C_T = 300\text{ pF}$ ,  $C_L = 1.0\text{ nF}$ . For typical values  $T_A = 25^\circ\text{C}$ , for min/max values  $T_A$  is the operating ambient temperature range that applies (Note 7), unless otherwise noted.)

Characteristic	Symbol	Min	Typ	Max	Unit
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## OSCILLATOR

Frequency (Error Amp Output Low) Total Variation ( $V_{CC} = 10\text{ V to }18\text{ V}$ , $T_A = T_{Low}$ to $T_{High}$ )	$f_{OSC(low)}$	490	525	550	kHz
Frequency (Error Amp Output High) Total Variation ( $V_{CC} = 10\text{ V to }18\text{ V}$ , $T_A = T_{Low}$ to $T_{High}$ )	$f_{OSC(high)}$	1850	2050	2200	kHz
Oscillator Control Input Voltage, Pin 3	$V_{in}$	–	2.5	–	V

## ONE-SHOT

Drive Output Off-Time $T_A = 25^\circ\text{C}$ Total Variation ( $V_{CC} = 10\text{ V to }18\text{ V}$ , $T_A = T_{Low}$ to $T_{High}$ )	$t_{Blank}$	235 225	250 –	270 280	ns
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## DRIVE OUTPUTS

Output Voltage Low State ( $I_{Sink} = 20\text{ mA}$ ) ( $I_{Sink} = 200\text{ mA}$ ) High State ( $I_{Source} = 20\text{ mA}$ ) ( $I_{Source} = 200\text{ mA}$ )	$V_{OL}$  $V_{OH}$	– – 9.5 9.0	0.8 1.5 10.3 9.7	1.2 2.0 – –	V
Output Voltage with UVLO Activated ( $V_{CC} = 6.0\text{ V}$ , $I_{Sink} = 1.0\text{ mA}$ )	$V_{OL(UVLO)}$	–	0.8	1.2	V
Output Voltage Rise Time ( $C_L = 1.0\text{ nF}$ )	$t_r$	–	20	50	ns
Output Voltage Fall Time ( $C_L = 1.0\text{ nF}$ )	$t_f$	–	15	50	ns

## FAULT COMPARATOR

Input Threshold	$V_{th}$	0.93	1.0	1.07	V
Input Bias Current ( $V_{Pin\ 10} = 0\text{ V}$ )	$I_{IB}$	–	–2.0	–10	$\mu\text{A}$
Propagation Delay to Drive Outputs (100 mV Overdrive)	$t_{PLH(In/Out)}$	–	60	100	ns

## SOFT-START

Capacitor Charge Current ( $V_{Pin\ 11} = 2.5\text{ V}$ )	$I_{chg}$	4.5	9.0	14	$\mu\text{A}$
Capacitor Discharge Current ( $V_{Pin\ 11} = 2.5\text{ V}$ )	$I_{dischg}$	3.0	8.0	–	mA

## UNDERVOLTAGE LOCKOUT

Startup Threshold, $V_{CC}$ Increasing Enable/UVLO Adjust Pin Open Enable/UVLO Adjust Pin Connected to $V_{CC}$	$V_{th(UVLO)}$	14.8 8.0	16 9.0	17.2 10	V
Minimum Operating Voltage After Turn-On, $V_{CC}$ Decreasing Enable/UVLO Adjust Pin Open Enable/UVLO Adjust Pin Connected to $V_{CC}$	$V_{CC(min)}$	8.0 7.6	9.0 8.6	10 9.6	V
Enable/UVLO Adjust Shutdown Threshold Voltage	$V_{th(Enable)}$	6.0	7.0	–	V
Enable/UVLO Adjust Input Current (Pin 9 = 0 V)	$I_{in(Enable)}$	–	–0.2	–1.0	mA

## TOTAL DEVICE

Power Supply Current (Enable/UVLO Adjust Pin Open) Startup ( $V_{CC} = 13.5\text{ V}$ ) Operating ( $f_{OSC} = 500\text{ kHz}$ ) (Note 6)	$I_{CC}$	– –	0.5 27	0.8 35	mA
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Product parametric performance is indicated in the Electrical Characteristics for the listed test conditions, unless otherwise noted. Product performance may not be indicated by the Electrical Characteristics if operated under different conditions.

- Maximum package power dissipation limits must be observed.
- Adjust  $V_{CC}$  above the Startup Threshold voltage before setting to 12 V.
- Low duty cycle pulse techniques are used during test to maintain junction temperature as close to ambient as possible.
- $T_{low} = 0^\circ\text{C}$  for MC34067  
=  $-40^\circ\text{C}$  for MC33067, NCV33067  
 $T_{high} = +70^\circ\text{C}$  for MC34067  
=  $+85^\circ\text{C}$  for MC33067, NCV33067

MC34067, MC33067, NCV33067

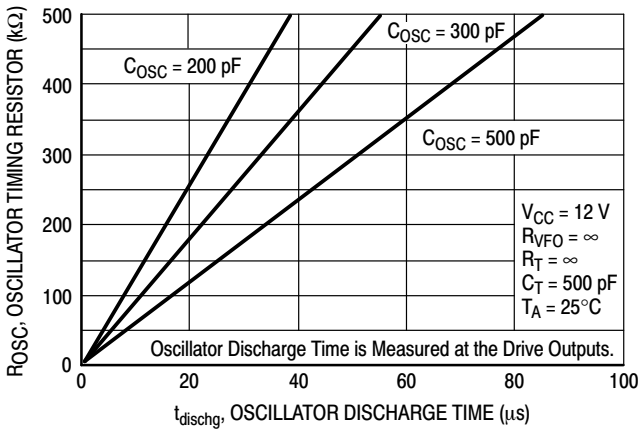


Figure 2. Oscillator Timing Resistor versus Discharge Time

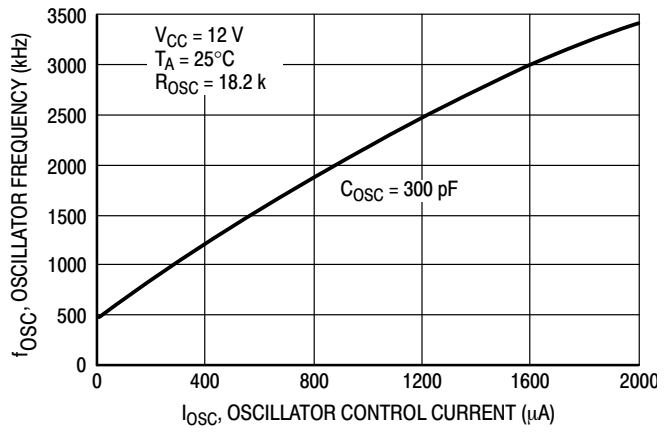


Figure 3. Oscillator Frequency versus Oscillator Control Current

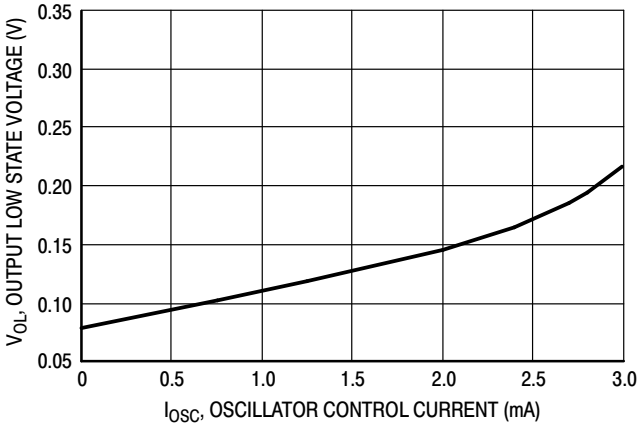


Figure 4. Error Amp Output Low State Voltage versus Oscillator Control Current

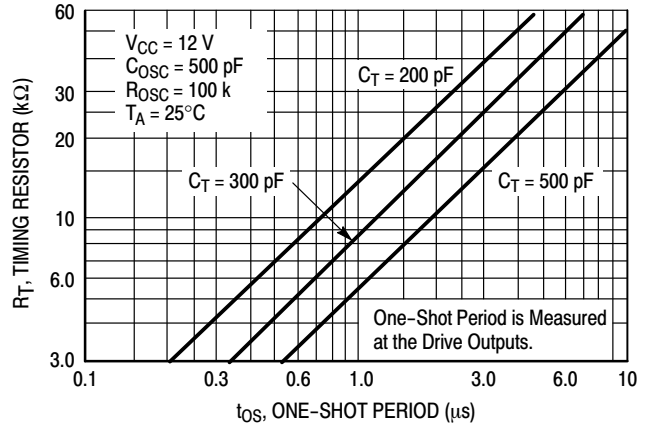


Figure 5. One-Shot Timing Resistor versus Period

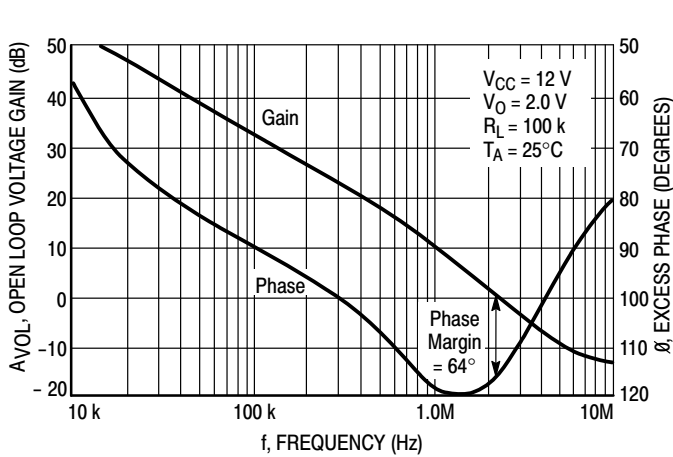


Figure 6. Open Loop Voltage Gain and Phase versus Frequency

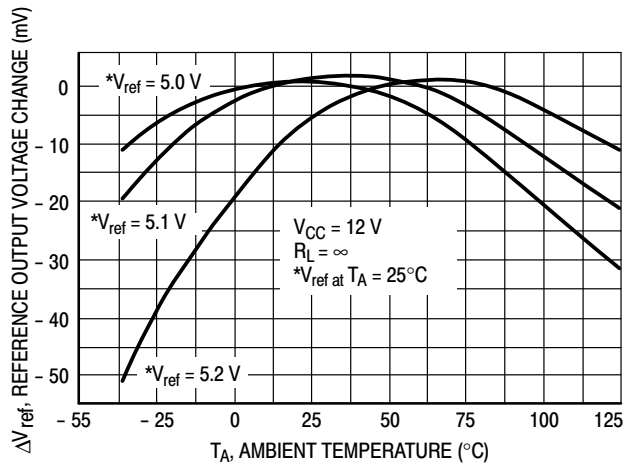


Figure 7. Reference Output Voltage Change versus Temperature

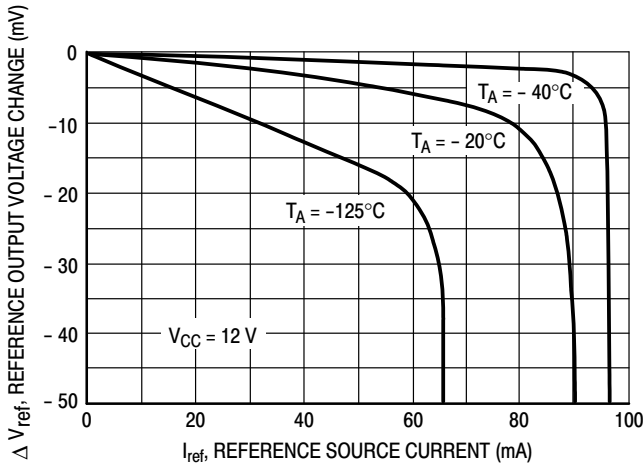


Figure 8. Reference Output Voltage Change versus Source Current

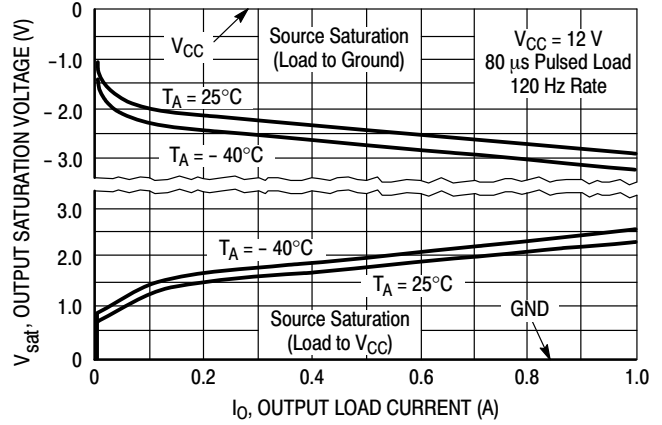


Figure 9. Drive Output Saturation Voltage versus Load Current

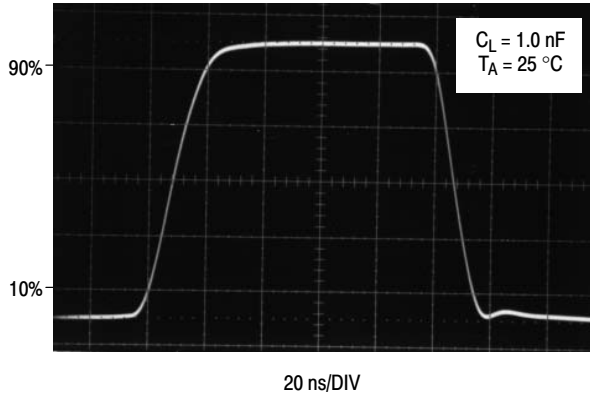


Figure 10. Drive Output Waveform

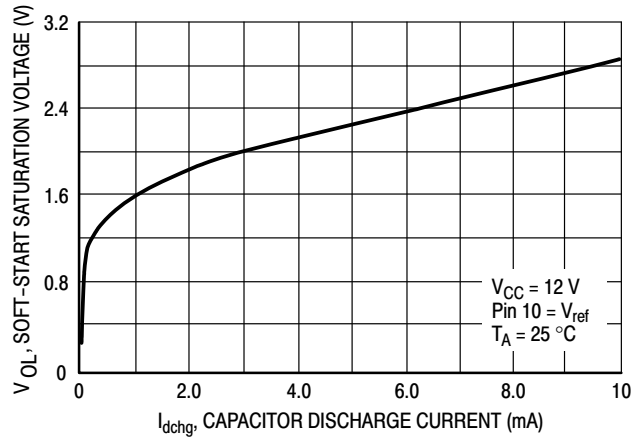


Figure 11. Soft-Start Saturation Voltage versus Capacitor Discharge Current

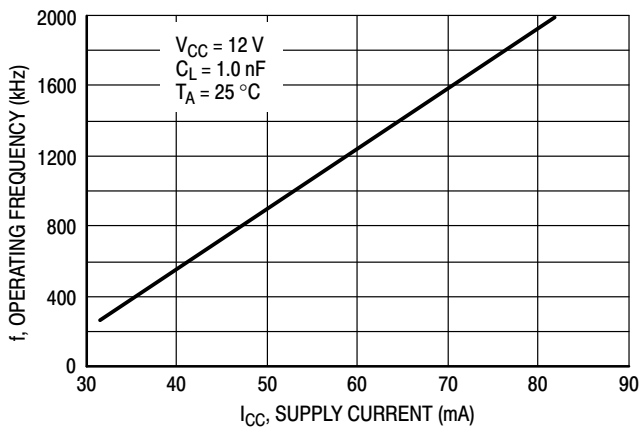


Figure 12. Operating Frequency versus Supply Current

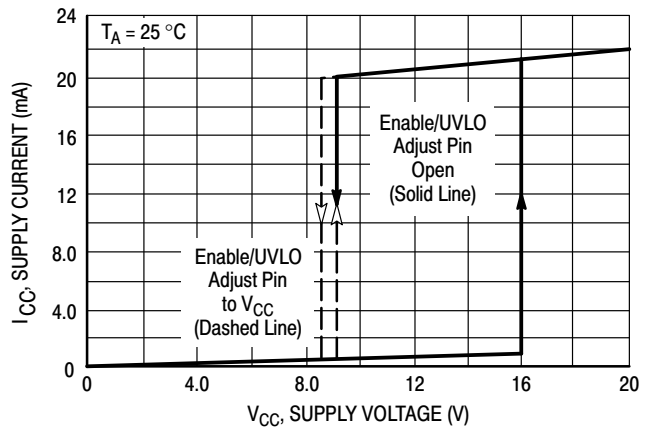


Figure 13. Supply Current versus Supply Voltage

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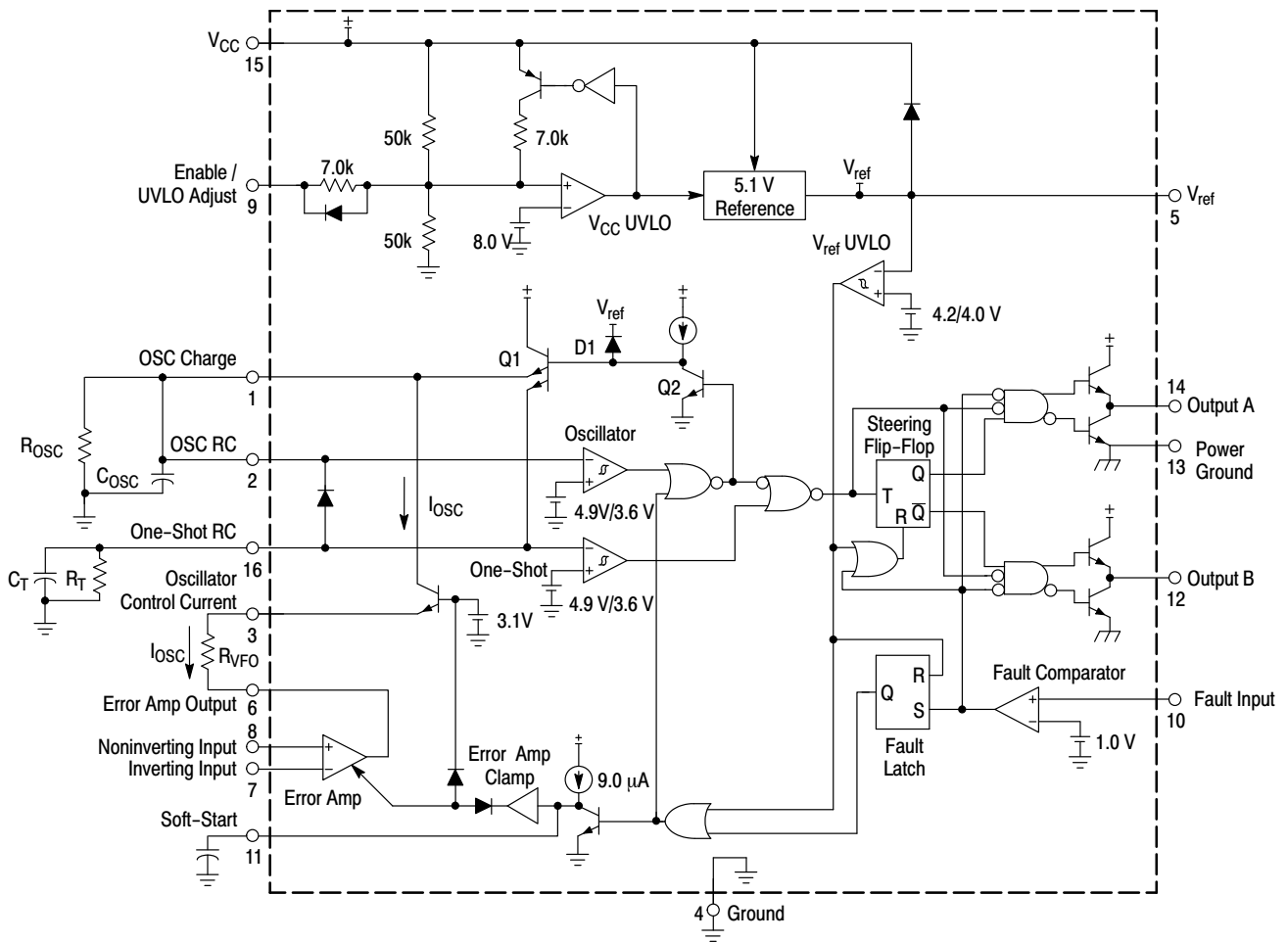


Figure 14. MC34067 Representative Block Diagram

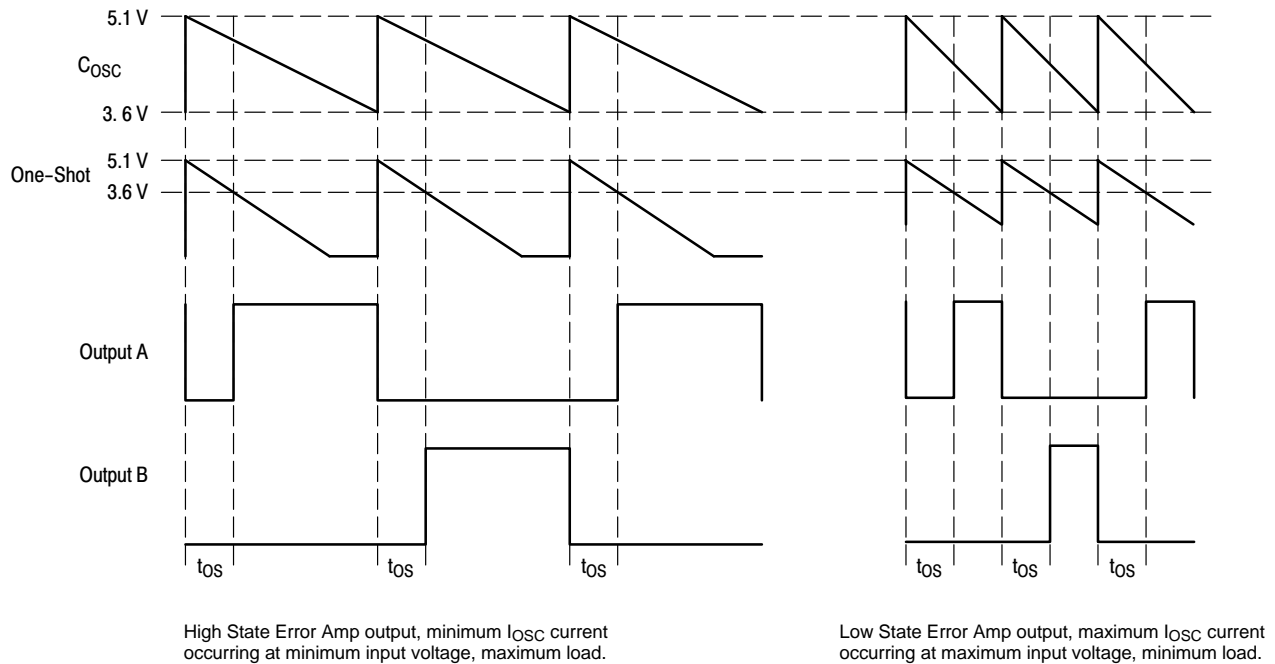


Figure 15. Timing Diagram



The minimum frequency is programmed by  $R_{OSC}$  using Equation 1:

$$R_{OSC} = \frac{\frac{1}{f_{(min)}} - t_{PD}}{C_{OSC} \ln\left(\frac{5.1}{3.6}\right)} = \frac{t_{(max)} - 70 \text{ ns}}{0.348 C_{OSC}} \quad (\text{eq. 1})$$

where  $t_{PD}$  is the internal propagation delay.

The maximum oscillator frequency is set by the current through resistor  $R_{VFO}$ . The current required to discharge  $C_{OSC}$  at the maximum oscillator frequency can be calculated by Equation 2:

$$I_{(max)} = C_{OSC} \frac{5.1 - 3.6}{\frac{1}{f_{(max)}}} = 1.5 C_{OSC} f_{(max)} \quad (\text{eq. 2})$$

The discharge current through  $R_{OSC}$  must also be known and can be calculated by Equation 3:

$$I_{R_{OSC}} = \frac{5.1 - 3.6}{R_{OSC}} \varepsilon \left( -\frac{1}{R_{OSC} C_{OSC} f_{(min)}} \right) \\ = \frac{1.5}{R_{OSC}} \varepsilon \left( -\frac{1}{f_{(min)} R_{OSC} C_{OSC}} \right) \quad (\text{eq. 3})$$

Resistor  $R_{VFO}$  can now be calculated by Equation 4:

$$R_{VFO} = \frac{2.5 - V_{EA\text{sat}}}{I_{(max)} - I_{R_{OSC}}} \quad (\text{eq. 4})$$

### One-Shot Timer

The One-Shot is designed to disable both outputs simultaneously providing a deadtime before either output is enabled. The One-Shot capacitor ( $C_T$ ) is charged concurrently with the oscillator capacitor by transistor Q1, as shown in Figure 16. The one-shot period begins when the oscillator comparator turns off Q1, allowing  $C_T$  to discharge. The period ends when resistor  $R_T$  discharges  $C_T$  to the threshold of the One-Shot comparator. The lower threshold of the One-Shot is 3.6 V. By choosing  $C_T$ ,  $R_T$  can be solved by Equation 5:

$$R_T = \frac{t_{OS}}{C_T \ln\left(\frac{5.1}{3.6}\right)} = \frac{t_{OS}}{0.348 C_T} \quad (\text{eq. 5})$$

Errors in the threshold voltage and propagation delays through the output drivers will affect the One-Shot period. To guarantee accuracy, the output pulse of the control chip is trimmed to within 5% of 250 ns with nominal values of  $R_T$  and  $C_T$ .

The outputs of the Oscillator and One-Shot comparators are OR'd together to produce the pulse  $t_{OS}$ , which drives the Flip-Flop and output drivers. The output pulse ( $t_{OS}$ ) is initiated by the Oscillator and terminated by the One-Shot comparator. With zero voltage resonant mode converters, the oscillator discharge time should never be set less than the one-shot period.

### Error Amplifier

A fully accessible high performance Error Amplifier is provided for feedback control of the power supply system. The Error Amplifier is internally compensated and features dc open loop gain greater than 70 dB, input offset voltage of less than 10 mV and a guaranteed minimum gain-bandwidth product of 2.5 MHz. The input common mode range extends from 1.5 V to 5.1 V, which includes the reference voltage.

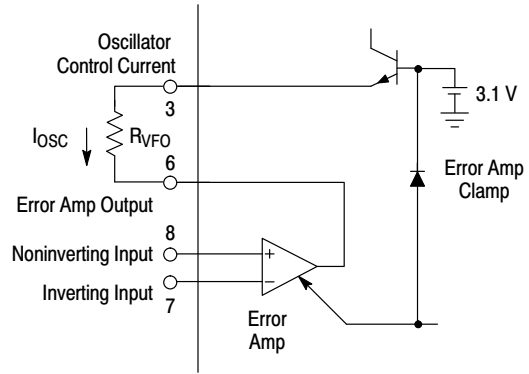


Figure 17. Error Amplifier and Clamp

When the Error Amplifier output is coupled to the  $I_{OSC}$  pin by  $R_{VFO}$ , as illustrated in Figure 17, it provides the Oscillator Control Current,  $I_{OSC}$ . The output swing of the Error Amplifier is restricted by a clamp circuit to improve its transient recovery time.

### Output Section

The pulse ( $t_{OS}$ ), generated by the Oscillator and One-Shot timer is gated to dual totem-pole output drives by the Steering Flip-Flop shown in Figure 18. Positive transitions of  $t_{OS}$  toggle the Flip-Flop, which causes the pulses to alternate between Output A and Output B. The flip-flop is reset by the undervoltage lockout circuit during startup to guarantee that the first pulse appears at Output A.

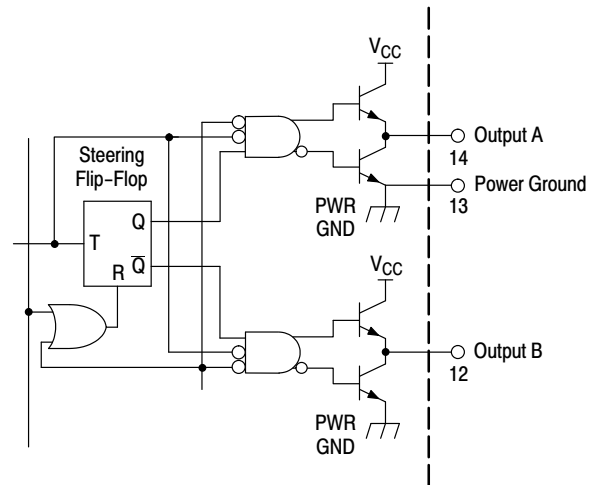


Figure 18. Steering Flip-Flop and Output Drivers



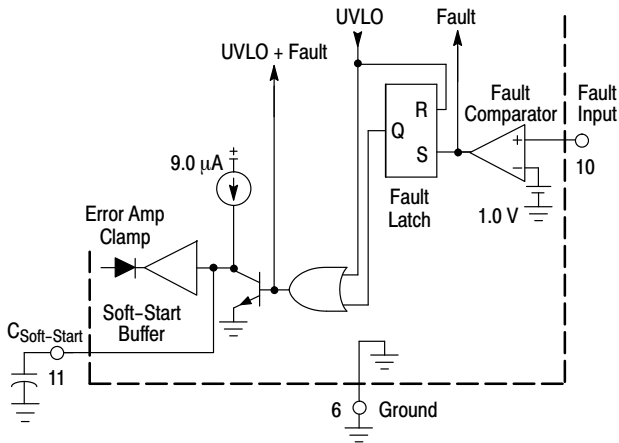


Figure 20. Fault Detector and Soft-Start

### Soft-Start Circuit

The Soft-Start circuit shown in Figure 20 forces the variable frequency Oscillator to start at the maximum frequency and ramp downward until regulated by the feedback control loop. The external capacitor at the  $C_{Soft-Start}$  terminal is initially discharged by the UVLO+Fault signal. The low voltage on the capacitor passes through the Soft-Start Buffer to hold the Error Amplifier output low. After UVLO+Fault switches to a logic zero, the soft-start capacitor is charged by a 9.0  $\mu$ A current source. The buffer allows the Error Amplifier output to follow the soft-start capacitor until it is regulated by the Error Amplifier inputs. The soft-start function is generally applicable to controllers operating below resonance and can be disabled by simply opening the  $C_{Soft-Start}$  terminal.

## APPLICATIONS INFORMATION

The MC34067 is specifically designed for zero voltage switching (ZVS) quasi-resonant converter (QRC) applications. The IC is optimized for double-ended push-pull or bridge type converters operating in continuous conduction mode. Operation of this type of ZVS with resonant properties is similar to standard push-pull or bridge circuits in that the energy is transferred during the transistor on-time. The difference is that a series resonant tank is usually introduced to shape the voltage across the power transistor prior to turn-on. The resonant tank in this topology is not used to deliver energy to the output as is the case with zero current switch topologies. When the power transistor is enabled the voltage across it should already be zero, yielding minimal switching loss. Figure 21 shows a timing diagram for a half-bridge ZVS QRC. An application circuit is shown in Figure 22. The circuit built is a dc to dc half-bridge converter delivering 75 W to the output from a 48 V source.

When building a zero voltage switch (ZVS) circuit, the objective is to waveshape the power transistor's voltage waveform so that the voltage across the transistor is zero when the device is turned on. The purpose of the control IC is to allow a resonant tank to waveshape the voltage across the power transistor while still maintaining regulation. This is accomplished by maintaining a fixed deadtime and by varying the frequency; thus the effective duty cycle is changed.

Primary side resonance can be used with ZVS circuits. In the application circuit, the elements that make the resonant tank are the primary leakage inductance of the transformer ( $L_L$ ) and the average output capacitance ( $C_{OSS}$ ) of a power MOSFET ( $C_R$ ).

The desired resonant frequency for the application circuit is calculated by Equation 6:

$$f_r = \frac{1}{2\pi\sqrt{L_L 2C_R}} \quad (\text{eq. 6})$$

In the application circuit, the operating voltage is low and the value of  $C_{OSS}$  versus Drain Voltage is known. Because the  $C_{OSS}$  of a MOSFET changes with drain voltage, the value of the  $C_R$  is approximated as the average  $C_{OSS}$  of the MOSFET. For the application circuit the average  $C_{OSS}$  can be calculated by Equation 7:

$$C_R = \sqrt{2} * C_{OSS} \text{ measured at } \frac{1}{2} V_{in} \quad (\text{eq. 7})$$

The MOSFET chosen fixes  $C_R$  and that  $L_L$  is adjusted to achieve the desired resonant frequency.

However, the desired resonant frequency is less critical than the leakage inductance. Figure 21 shows the primary current ramping toward its peak value during the resonant transition. During this time, there is circulating current flowing through the secondary inductance, which effectively makes the primary inductance appear shorted. Therefore, the current through the primary will ramp to its peak value at a rate controlled by the leakage inductance and the applied voltage. Energy is not transferred to the secondary during this stage, because the primary current has not overcome the circulating current in the secondary. The larger the leakage inductance, the longer it takes for the primary current to slew. The practical effect of this is to lower the duty cycle, thus reducing the operating range.

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The maximum duty cycle is controlled by the leakage inductance, not by the MC34067. The One-Shot in the MC34067 only assures that the power switch is turned on under a zero voltage condition. Adjust the one-shot period

so that the output switch is activated while the primary current is slewing but before the current changes polarity. The resonant stage should then be designed to be as long as the time for the primary current to go to 0 A.

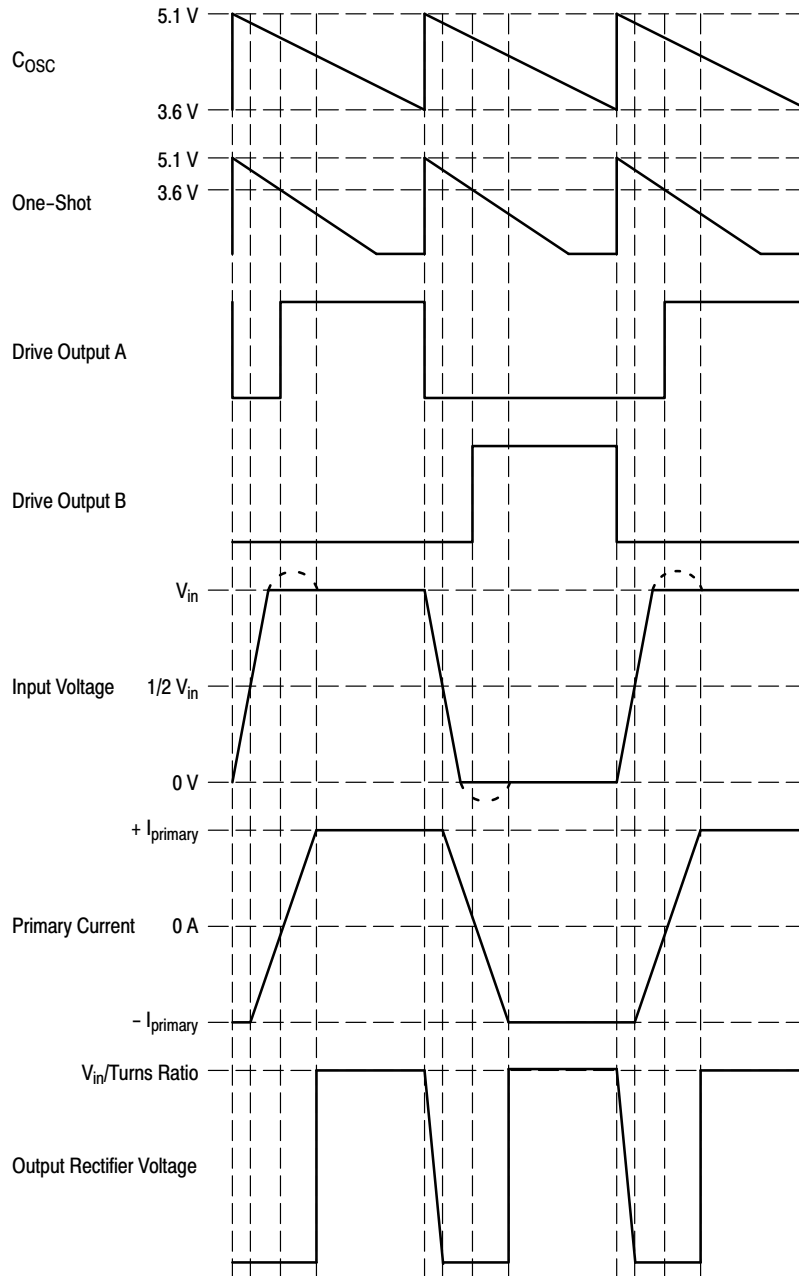
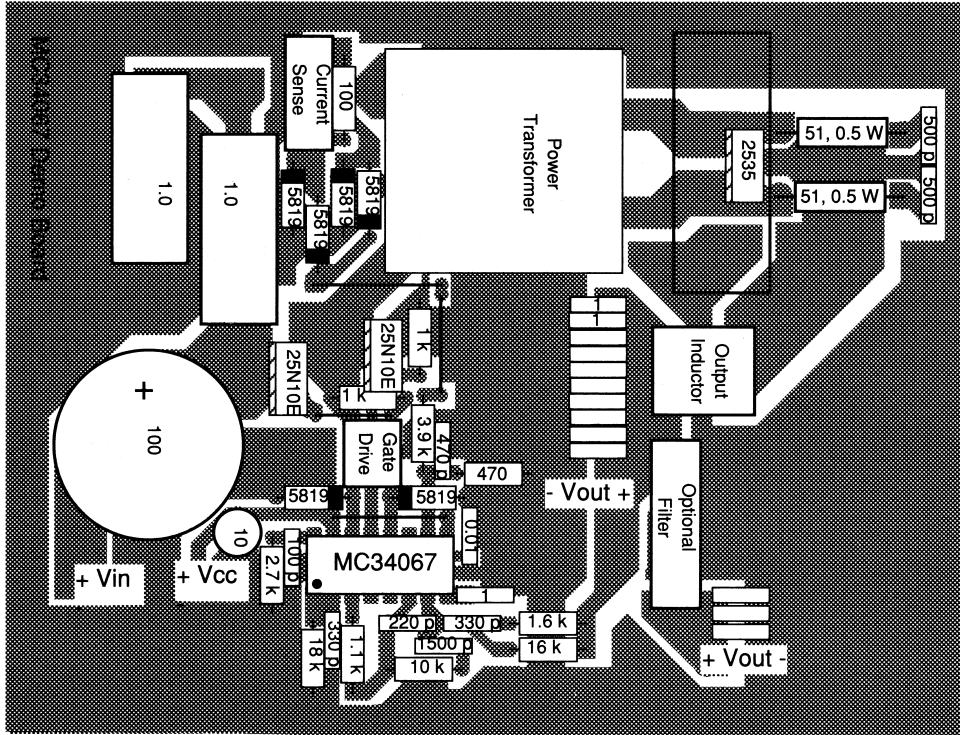


Figure 21. Application Timing Diagram



# MC34067, MC33067, NCV33067

(Top View)



(Bottom View)

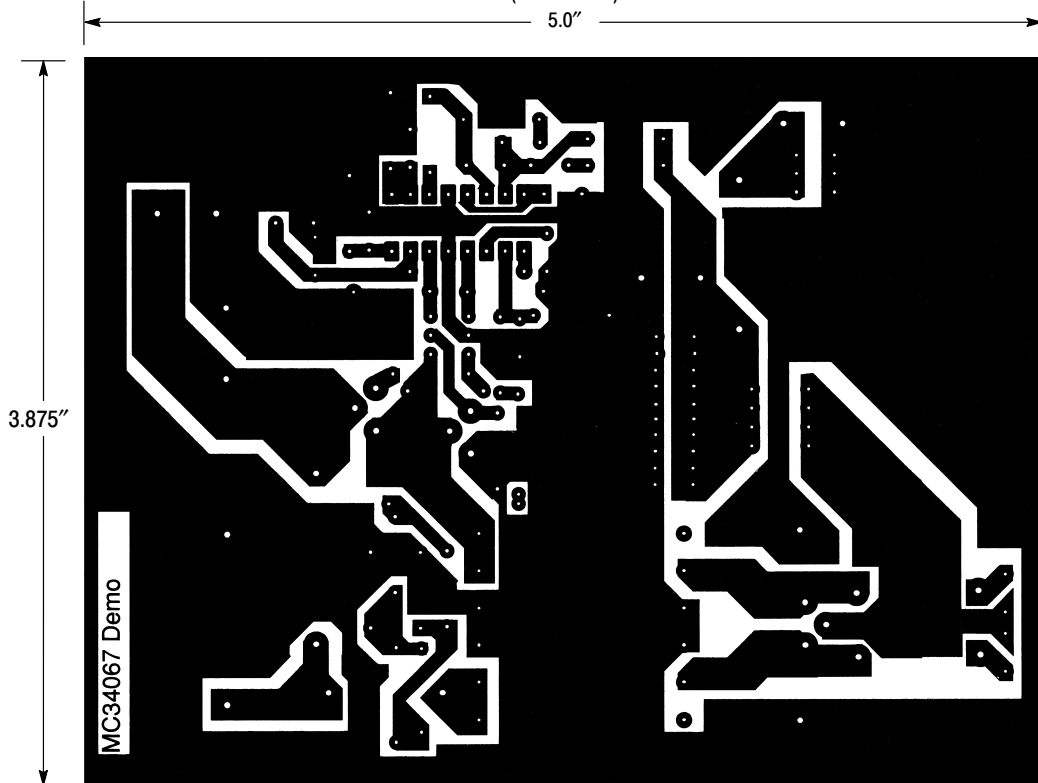
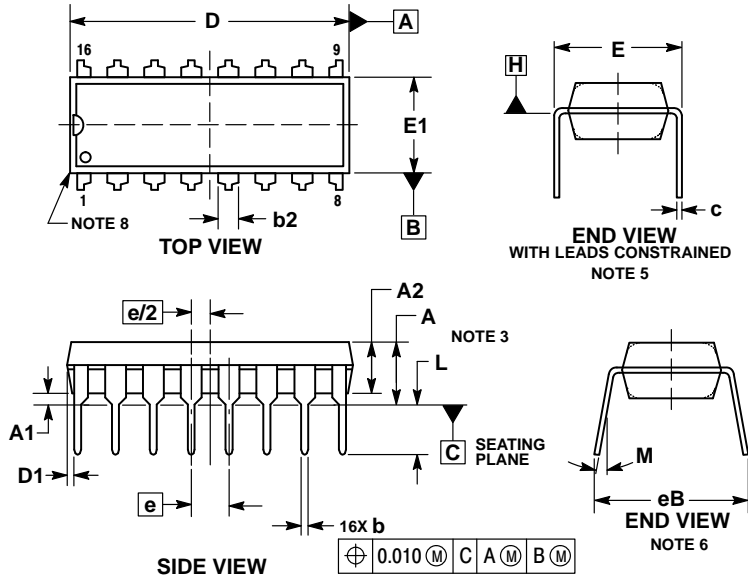


Figure 23. Printed Circuit Board and Component Layout

# MC34067, MC33067, NCV33067

## PACKAGE DIMENSIONS

PDIP-16  
P SUFFIX  
CASE 648-08  
ISSUE U



NOTES:

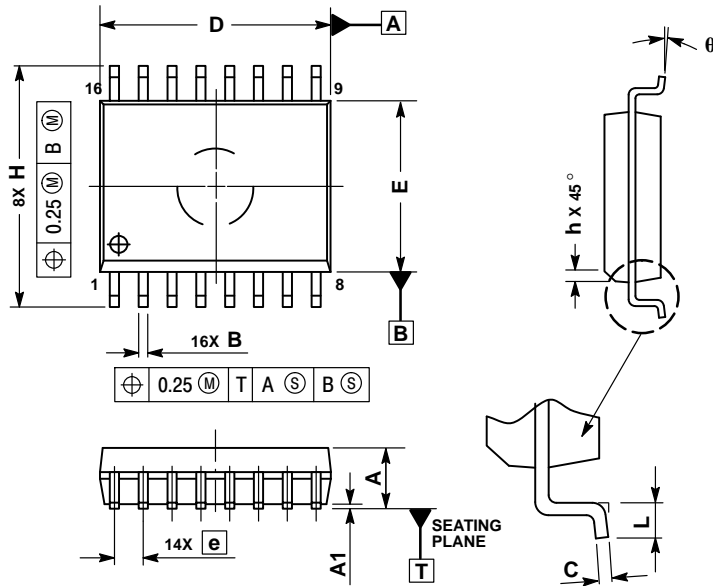
1. DIMENSIONING AND TOLERANCING PER ASME Y14.5M, 1994.
2. CONTROLLING DIMENSION: INCHES.
3. DIMENSIONS A, A1 AND L ARE MEASURED WITH THE PACKAGE SEATED IN JEDEC SEATING PLANE GAUGE GS-3.
4. DIMENSIONS D, D1 AND E1 DO NOT INCLUDE MOLD FLASH OR PROTRUSIONS. MOLD FLASH OR PROTRUSIONS ARE NOT TO EXCEED 0.10 INCH.
5. DIMENSION E IS MEASURED AT A POINT 0.015 BELOW DATUM PLANE H WITH THE LEADS CONSTRAINED PERPENDICULAR TO DATUM C.
6. DIMENSION E3 IS MEASURED AT THE LEAD TIPS WITH THE LEADS UNCONSTRAINED.
7. DATUM PLANE H IS COINCIDENT WITH THE BOTTOM OF THE LEADS, WHERE THE LEADS EXIT THE BODY.
8. PACKAGE CONTOUR IS OPTIONAL (ROUNDED OR SQUARE CORNERS).

DIM	INCHES		MILLIMETERS	
	MIN	MAX	MIN	MAX
A	---	0.210	---	5.33
A1	0.015	---	0.38	---
A2	0.115	0.195	2.92	4.95
b	0.014	0.022	0.35	0.56
b2	0.060 TYP		1.52 TYP	
C	0.008	0.014	0.20	0.36
D	0.735	0.775	18.67	19.69
D1	0.005	---	0.13	---
E	0.300	0.325	7.62	8.26
E1	0.240	0.280	6.10	7.11
e	0.100 BSC		2.54 BSC	
eB	---	0.430	---	10.92
L	0.115	0.150	2.92	3.81
M	---	10°	---	10°

# MC34067, MC33067, NCV33067

## PACKAGE DIMENSIONS

**SOIC-16W**  
**DW SUFFIX**  
 CASE 751G-03  
 ISSUE D

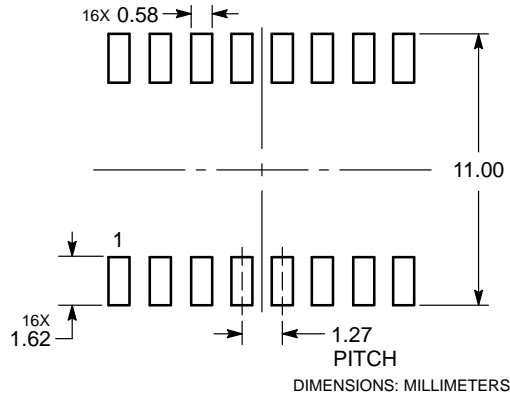



**NOTES:**

1. DIMENSIONS ARE IN MILLIMETERS.
2. INTERPRET DIMENSIONS AND TOLERANCES PER ASME Y14.5M, 1994.
3. DIMENSIONS D AND E DO NOT INCLUDE MOLD PROTRUSION.
4. MAXIMUM MOLD PROTRUSION 0.15 PER SIDE.
5. DIMENSION B DOES NOT INCLUDE DAMBAR PROTRUSION. ALLOWABLE DAMBAR PROTRUSION SHALL BE 0.13 TOTAL IN EXCESS OF THE B DIMENSION AT MAXIMUM MATERIAL CONDITION.

MILLIMETERS		
DIM	MIN	MAX
A	2.35	2.65
A1	0.10	0.25
B	0.35	0.49
C	0.23	0.32
D	10.15	10.45
E	7.40	7.60
e	1.27 BSC	
H	10.05	10.55
h	0.25	0.75
L	0.50	0.90
q	0°	7°

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